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The Proceedings of 2022 International Conference on Wireless Power Transfer (ICWPT2022)

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Contents

Quadrature Six-Coils Wireless Charging with High Misalignment Tolerance and Constant Voltage Output	1
<i>Zhaowei Gong, Jingang Li, Xiangqian Tong, and Ningchao Zhang</i>	
Inductively Coupled Power Transfer System Based Constant Voltage and Constant Current Charging for Rail Transit System	8
<i>Jixin Yang, Liming Shi, Zhenggang Yin, and Wenjing Tang</i>	
Modeling and Analysis of Bidirectional Wireless Power Transfer System with Asymmetric Parameters	18
<i>Chenyang Wei, Bin Wei, Cheng Jiang, and Xiaokang Wu</i>	
Design and Research on Coupling Mechanism of Inductive Power Transmission	29
<i>Wei Liu, Liangshun Sun, Mingwei Su, Fangrui Wang, Jian Long, Enxin Xiang, and Longlei Bai</i>	
Characteristics of Wireless Power Transmission Based on a New Spiral Resonant Coil	36
<i>Haoyan Xi, Yihao Wei, Yong Dong, Yanhong Liu, Lijuan Dong, and Yunlong Shi</i>	
Efficiency Optimization Method for Wireless Power Transfer System Between the Rocket and the Ground Based on Energy Compensation	45
<i>Zhan Wang, Kun Lan, Jingang Zhang, and Da Yu</i>	
Design and Modeling of Helmholtz Coil Based on Winding Method Optimization	57
<i>Xueting Zhao, Zihao Zhang, Xiaoyun Chen, Yi Zhou, and Deyan Lin</i>	
Applicability Analysis of Coupled-Mode Theory Model in Capacitive Power Transfer System	71
<i>Yang Zhou, Jingjing Yang, Yiming Zhang, Qingbin Chen, and Yanwei Jiang</i>	
Optimal Efficiency Control of Multiple Transmitting Array WPT System for Constant Power	81
<i>Boxiang Sun, Shui Pang, Jiayi Xu, Hongyu Li, and Xingfei Li</i>	

Optimized Design of the DD Coil for Improved Misalignment Tolerance	91
<i>Wei jie Li, Wei yao Mei, Jiangjun Yuan, Zhonghao Dongye, and Lijun Diao</i>	
Analysis of Geometric Characteristics of Three-Terminal Shaft Loosely Coupled Transformer Based on LCC-S Compensation	99
<i>Shijia Kang, Zewen Wang, Zijia Zhang, Yansong Li, and Jun Liu</i>	
Frequency Tracking Synchronization Technique for a Bidirectional Inductive Power Transfer System	107
<i>Bowang Zhang, Wei Han, Youhao Hu, and Weikang Hu</i>	
Analysis and Design of Magnetic Cores for Rotary Wireless Power Transfer Applications	117
<i>Longyuan Fan, Zicheng Liu, Jiewei He, and Dong Jiang</i>	
Electrical Characteristics of Magnetic Couplers in Inductive Power Transfer for Autonomous Underwater Vehicles	128
<i>Jiangjun Yuan, Wei yao Mei, Quan Yuan, Zhonghao Dongye, and Lijun Diao</i>	
Generation of an Airy Beam Based on a Holographic Scalar Metasurface	138
<i>Song Zhang, Hao Xue, Xiaonan Wu, Mingyang Chang, and Long Li</i>	
Modulation of Deflected Bessel Beams Based on Reconfigurable Metasurface	145
<i>Shihao Zhao, Hao Xue, Song Zhang, Mingyang Chang, and Long Li</i>	
Simulation and Optimization Analysis of Magnetic Coupling Mechanism for Resonant Wireless Power Transfer	153
<i>Junjie Guo, Tao Ning, Kaijian Zhang, Xiaodong Zhang, Yuling Ma, and Yijia Shang</i>	
Loss Analysis of Rectifier Circuit and Its Optimization Technique in Wireless Power Transfer System	166
<i>Xu Zhang, Qingbin Chen, and Wei Chen</i>	
Simultaneous Wireless Power and Data Transfer System Using Parallel Injection Communication Method	177
<i>Guangjie Bao and Linlin Tan</i>	
A Magnetic Field Energy Harvester to Power Micro-power Sensors on the Freight Train for Railway Application	190
<i>Jin Tao, Bo Luo, Yongchao Wang, Zhuling Wang, and Ruikun Mai</i>	

Coupling Comparison of Magnetic Couplers for Mid-range Wireless Power Transfer Systems	199
<i>Yousu Yao, Zixu Fang, Qinan Ni, and Xiufang Liu</i>	
Model-Inverse-Based Output Control of the Multi-excitation-Unit WPT System	210
<i>Xiao Lv, Zi-yi Xia, Du-gang Kang, and Xin Dai</i>	
The Impact of Metal Hull of AUVs for Underwater Wireless Power Transfer System	218
<i>Lei Yang, Yuanqi Zhang, Xiaojie Li, Baoxiang Feng, Jingjing Huang, Darui Zhu, Aimin Zhang, and Xiangqian Tong</i>	
Synchronous Identification of Loads and Mutual Inductances for Multi-frequencies Multi-loads WPT System	229
<i>Dongxiao Huang, Qinwang Wei, Weidong Huang, Zequan Hong, and Fengxiang Wang</i>	
A Cross-Shaped Solenoid Magnetic Coupler with High Lateral Offset Tolerance	239
<i>Chendawei Zhang, Wenzhou Lu, Jian Zhao, Qigao Fan, and Haiying Chen</i>	
A Design of Secondary-Only Resonant Series-Series WPT System to Maintain Power Stability with Coil Misalignment	247
<i>Yueyao Li, Xiaohua Wu, and Xiliang Chen</i>	
Research on Constant Voltage Control Strategy of Dual Pick-Up Dynamic Inductive Coupled Power Transfer System Based on Optimal Efficiency	255
<i>Anran Sun and Chenyang Xia</i>	
Analysis and Modeling of Response Characteristics Under Actual Rectifier Parameters in the Wireless Power Transfer System	264
<i>Binzhi Xie, Jinshuai Wang, Zhibin Lu, Wei Chen, and Qingbin Chen</i>	
Metal Object Detection for Electric Vehicle Wireless Charging Based on Fusion of Spectral and Texture Features	277
<i>Zengpeng Zhou, Jindong Tian, Bo Liu, and Yong Tian</i>	
Study on the Performance of a Novel High Lateral Displacement Receiver Coil Based on Cross-Winding Method	287
<i>Chang Liu, Jinhai Jiang, Kai Song, Xiaoyan Li, Jianing Xu, and Chunbo Zhu</i>	

Anti-misalignment Improvement for SS Compensated IPT System Using Reconfigurable Rectifier	299
<i>Yang Chen, Xiaofei Lyu, Yuhua Xiao, Xize Jiao, and Ruikun Mai</i>	
Design and Icing Analysis of a Novel Magnetic Coupling Mechanism for WPT System on High-Voltage Transmission Lines	308
<i>Shuyu Shen, Linlin Tan, Zhijun Wu, Heqi Xu, Tian Gao, and Xueliang Huang</i>	
Research on Maximizing the Communication Capacity of OFDM-Based Simultaneous Wireless Transmission of Power and Information (SWTPI)	323
<i>Li Ji, Kaixin Yan, and Xudong Cao</i>	
Loss Analysis of Magnetic Core and Its Structure Optimization of Magnetic Coupling Structure in Wireless Power Transfer System	331
<i>Yujie Lan, Feng Fan, Xiaolong Deng, Wei Chen, and Qingbin Chen</i>	
Compact Mixed DC-DC Power Converters for Computing Server	341
<i>Zhiqiang Liu, Chaoqiang Jiang, Tianlu Mau, Jingchun Xiang, and Xiaosheng Wang</i>	
A Flexible Foreign Object Detection Method Based on Arrayed Vertical-Decoupled Coils for Wireless Power Transfer Systems	352
<i>Huishu Song, Xiaosheng Huang, Shuyi Lin, Ruping Lin, and Jing Huang</i>	
Optimal Efficiency Design of Single-to-Multiple Constant Voltage Based on LCC Compensation Topology for Wireless Power Transfer	364
<i>Cang Liang, Renjie Zhang, Cheng Zhao, Huan Yuan, Aijun Yang, Xiaohua Wang, and Mingzhe Rong</i>	
Design of Dynamic Wireless Charging System Based on Coupling Coefficient Estimation	372
<i>Xuchi Xue, Zhitao Liu, Jia Liu, Wenjie Chen, and Hongye Su</i>	
Influence of Frequency on Transmission Performance of Multi-relay Wireless Power Supply System	385
<i>Zhijun Wu, Linlin Tan, Shuyu Shen, and Heqi Xu</i>	
Bidirectional Wireless Power Transfer System Control Strategy on Double-Sided LCC Resonant Network	400
<i>Shuxuan Zheng, Kainan Chen, Yuchen Chen, Liqiang Yuan, and Zhengming Zhao</i>	

Design of Underwater Wet Plug Connectors System Based on the Principle of Wireless Power Transfer	415
<i>Jianduo Zhang, He Yin, Yudong Fu, Hai Lan, and Dan Li</i>	
Metal Foreign Object Detection Algorithm Based on Multivariate Normal Distribution	427
<i>Ying Sun, Kai Song, Tian Zhou, Guo Wei, and Chunbo Zhu</i>	
Research on Parallel Circulation Suppression Strategy of High-Frequency Resonant Inverter Based on Improved Active Current Decomposition Method	436
<i>Junfeng Liu, Mingze Ma, Hao Zhou, and Jun Zeng</i>	
The Power Control of a Multiple Pick-Up Bidirectional Wireless Power Transfer System	444
<i>Zhenggang Yin, Liming Shi, Jixin Yang, and Wenjing Tang</i>	
Robust Regulation of Constant Current Wireless Charging System with Clamping Coil	455
<i>Le Li, Bing Cheng, Houxuan Liu, Liangzong He, Wei Li, Tiejun Ma, and Yongjun Wang</i>	
Comparison of Wireless Power Transfer Systems with Multi-loads	463
<i>Wei Deng, Zhiliang Yang, Jing Yin, Jie Wu, Pengfei Gao, Yafei Chen, and Zhanshi Lou</i>	
Multi-objective Optimization of IPT System Compensation Parameters for Improving Misalignment Tolerance	472
<i>Junfeng Yang, Junjie Guo, Qingbin Tong, Xu Yang, and Tianqi Hao</i>	
Design of LCLC-S Impedance Matching Network for Ultrasonic Wireless Power Transmission System	482
<i>Kehan Zhang, Jiaming Feng, Baobao Lan, Xinyang Li, Zhengchao Yan, and Zhaoyong Mao</i>	
A Switchable Modular AC~DC Buck-Boost Converter for the Wide Input Range in Energy Harvesting	496
<i>Chunlong Li, Dengfeng Ju, Hui Huang, Kuan Ye, Hongjing Liu, and Jiayong Yuan</i>	
Research on Active Leakage Magnetic Field Suppression Techniques Applied in Electric Vehicle Wireless Chargers	506
<i>Ning Zhang, Xiaomin Zhou, Xianfeng Gong, Dawei Gao, and Guodong Zhu</i>	

The Solution of Power Frequency Electromagnetic Field for Parallel Transmission Lines Based on Superposition Algorithm	516
<i>Jiangong Zhang, Xiaofeng Yang, Zheyuan Gan, Zhibin Zhao, and Bo Tang</i>	
Coupler Comparison of Inductive and Capacitive Power Transfer Systems	523
<i>Siyi Yao, Minfan Fu, Heyuan Li, Yiming Yin, and Peng Zhao</i>	
Design of Integrated Coil Structure for Simultaneous Wireless Information and Power Transfer Applied to Electric Power Inspection Robot	531
<i>Chen Huang, Nenghong Xia, Xike Mao, Chengchao Hua, Xiaoying Xu, and Zhipeng Yuan</i>	
Reconfiguration and Reuse of Receiver/Repeater in Wireless Power Transmission System	543
<i>Han Liu, Lingling Sun, and Wei Zhang</i>	
Improved Electromagnetic Halbach Array for Enhanced Efficiency in Wireless Power Transfer	550
<i>Dibin Zhu and Tamuno-omie Gogo</i>	
Robust Control of Ultrasonic Power Transfer System Under Parameter Perturbation	559
<i>Kehan Zhang, Baobao Lan, Fan Dai, Jiaming Feng, and Zhaoyong Mao</i>	
Influence of Loop Impedance on Performance of Charging Power Supply Based on Battery Packs Connected in Series	571
<i>Shikuo Cheng, Yinghui Gao, Jing Han, Kun Liu, Yaohong Sun, and Ping Yan</i>	
Current Source Converter Optimization Method Based on Multi-step FCS-MPC	583
<i>Hao Ding, Quanjie Li, Mingming Li, and Wei Wang</i>	
A Fixed-Admittance Modeling Method of Power Electronic Switches Based on State Initializations	592
<i>Bin Zhou, Guangsen Wang, Weichao Li, Kang Wang, and Guisheng Jie</i>	
Configuration Strategies of Reactive Power Compensation in Converter Stations with STATCOM	604
<i>Kanglong Yuan, Mingyu Han, Huansheng Zhou, Yan Li, Yu Huang, and Yu Liang</i>	

SiC MOSFET Gate Drive Power Supply Based on Active Clamp Flyback	614
<i>Dahan Deng, Jingwei Zhang, and Shuhao Li</i>	
Analysis of Release Voltage Fluctuation Mechanism of Electromagnetic Relay with Bridge Polarized Magnetic System	623
<i>Guilin Liu, Yong Xie, Huimin Liang, Zitong Wei, Junfeng Chen, and Manyun Huang</i>	
Analysis and Optimization of a Three-Coil Coupler Based WPT System Featuring High Efficiency and Misalignment Tolerance	632
<i>Yousu Yao, Chunxu Zhang, and Qinan Ni</i>	
Research on Interleaved DC-DC Converter with Extended CD Unit	643
<i>Rui Guo, Sen Yang, and Liying Jiang</i>	
Double Random PWM Method of DC-DC Chopper Converter Based on WELL Look-Up Table Method	651
<i>Guohua Li, Guangda Liu, and Yang Liu</i>	
Design and Analysis of a High-Voltage and High-Power ANPC Three-Level Power Module	662
<i>Yichun Zhang, Zechun Dou, Hangjie Fu, Jiayi Wang, Xiongbo Xie, and Yanping Chen</i>	
Research on the Influence of Cable Capacitance of EMU Converter on IGBT Protection and Control	673
<i>Jianguang Yang, Jun Liao, Hangjie Fu, Mingyi Chen, and Shunmeng Xie</i>	
Optimal Sampling Frequency of SVPWM for Multilevel Converter	683
<i>Wenjun Zeng, Cui Wang, Qiangsheng Dai, Zhanhao Zhao, Chenhang Wu, Zuojia Niu, and Haoran Li</i>	
Reliability Evaluation Method of Active Distribution Network Based on Optimization Model	692
<i>Feng Zhao, Youzhong Miao, Chao Sun, Jing Wang, and Zongmin Yu</i>	
A Review of the Current State of Development of High Precision AC Power Frequency Converter	701
<i>Ruiqi Zhang, Li Liu, and Xiaohui Zhang</i>	
Electromagnetic Scattering Characteristics of Different Polarized Electromagnetic Waves by High Voltage Transmission Lines	714
<i>Xianglin Ma, Yanxia Lu, Chaoqun Jiao, Jianggong Zhang, Zhibin Zhao, and Zheyuan Gan</i>	

The Acquisition and Research of the Relative Complex Permeability of the Core Material of the Self-inductive Displacement Sensor	723
<i>Zongqiang Ren, Xinwei Chen, Hongwei Li, and Wentao Yu</i>	
Current Sharing of Parallel IGBT Affected by Thermal Resistance	731
<i>Weifeng Tang and Changjiang Wang</i>	
A Novel High Step-up DC-DC Converter Integrating Coupled-Inductor with Quasi-Symmetric Gain Feature	739
<i>Yihai Li, Yan Zhang, and Jinjun Liu</i>	
A Behavior Model of Planar SiC MOSFET Considering Avalanche Breakdown	748
<i>Yifan Wu, Chi Li, Zedong Zheng, Lianzhong Wang, Tao Liu, and Guojing Liu</i>	
Envelope Tracking Power Supply for Energy Saving of Mobile Communication Base Stations	766
<i>Xiaoguang Gao, Hao Wang, Linguo Wang, and Bin Zhang</i>	
Calculation of Turn-To-Turn Parasitic Capacitance	775
<i>Hao Wang, Peng Zhou, Zenan Xu, Zhijun Ye, Kaixiang Chen, Zongxuan Ma, and Jiliang Luo</i>	
A Lag Compensation Method Based on All-Pass Filter	784
<i>Zhang Hongzhen, Hou Shiyong, Robert M. Cuzner, and Ye Jiangdan</i>	
Characteristic Research of Magnetic Controllable Voltage Regulator	793
<i>Guosheng Zhao, Xiaolei Zheng, Junpeng Pan, and Xiaohuan Hu</i>	
Space Vector Pulse Width Modulation Strategy for Cascaded Three-Phase Bridge Converters	801
<i>Yunhe Wang, Cui Wang, Qiangsheng Dai, Zhanhao Zhao, Chenhang Wu, Zuoja Niu, and Haoran Li</i>	
Design and Optimization of Totem Pole Bridgeless PFC Based on GaN	810
<i>Mengyang Tang, Pengfei Xue, Zhangge Cheng, and Tao Yong</i>	
A Modular Multi-port Converter for Distribution of Vessel Integrated Power System	819
<i>ZhaoJie Huang, Qiang Ren, Fei Xiao, JiLong Liu, and ZhiChao Zhu</i>	
Configuration Method and Parameter Impact Analysis of Parallel LCC Compensation WPT Systems	829
<i>Chao Cui, Xin Gao, Shumei Cui, and Qianfan Zhang</i>	

Design and Comparative Analysis of Symmetric and Asymmetric Couplers for Underwater Wireless Power Transmission System	843
<i>Jiacheng Li, Jianing Feng, Xun Dou, Hanyu Yang, Xin Zhang, and Kai Ni</i>	
Comparison and Analysis of Common Electromagnetic Field Numerical Computation Methods in Cable Model	852
<i>Yanxin Ren, Nana Duan, Xinyu Ma, Weijie Xu, and Shuhong Wang</i>	
Research and Design of Active Clamp Forward Converter	861
<i>Wang Zhou, Gaili Yue, Zijing Wang, Jiadong Yao, and Wenjie Gao</i>	
Development of Calibration Device for Transformer Winding Deformation Tester	870
<i>Pengfei Shi, Xuefang Luo, and Dazhi Ni</i>	
A Novel APSO-GA Specific Harmonic Elimination Method for Nine Level Inverter	877
<i>He Qiao, Ziqi Zhao, and Zhaohui Shen</i>	
Suppression Method of DC Voltage Pulsation in Three - Phase Four - Wire APF	893
<i>Haihong Huang, Weijie Zhao, and Haixin Wang</i>	
Energy Coordinated Control Method for High Power Density Power Electronic Transformers	901
<i>Ziqing Cao, Yichao Sun, Liye Wu, Yinyu Yan, and Kai Yang</i>	
Effects of Magnetic Field Shielding on UED Ultrashort Electron Pulses	909
<i>Mengchao Li, Xuan Wang, Chuicai Rong, Wei Chen, Teng Gong, Menghao Tan, Jun Huang, and Xingquan Wang</i>	
Asymmetric Five-Switch Cascaded Multilevel Inverter and Its Modulation Strategy	916
<i>Fei He and Wei Sun</i>	
Impedance Measurement Method for Obtaining the Accuracy of Current Transformers	929
<i>Hongsen You, Mengying Gan, Dapeng Duan, Cheng Zhao, Yuan Chi, Weiqiong Song, Fengming Lv, Jinjun Xie, and Jiansheng Yuan</i>	
Fault Diagnosis Method of Cascaded H-Bridge Inverter Based on EEMD-MPE	938
<i>Weiman Yang, Weinian Wang, Xingguai Wang, and Xue Sheng</i>	

Development of All SiC EMU Charger Based on Vienna Rectifier	951
<i>Haiyang Li, Xuqiang Zhao, and Bowei Zhu</i>	
Research on Isolated DC/DC Converter with Frequency and Phase-Shift Adjustment Control Based on SiC Switches	962
<i>Nan Zhao, Zedong Zheng, and Yongdong Li</i>	
Design of Increasing Dielectric Constant of Metallized Film Capacitor to Reduce Its Volume in MMC	975
<i>Hongyu Yu, Li Ran, Hao Feng, and Jinxiao Wei</i>	
Prediction of Submarine Cable Probe Values Based on GA-BP Neural Network and Random Forest	983
<i>Shaohua Chen, Dingcheng Guo, Qingyi Cui, Sitong Yi, and Jiameng Li</i>	
Research on High Gain Quadratic Boost Converter with Coupled Inductors	992
<i>Rui Guo, Liying Jiang, and Sen Yang</i>	
A Simple and Effective Identification Method for Transient Pulse Wave Propagation Resulted from Overhead Transmission Line Fault	1004
<i>Yue Yu, Longhao Liu, Zexin Zhou, Zhanpeng Du, Dingyu Qin, and Chongqing Jiao</i>	
Multilevel Pulse Train Control Three-Phase Inverter Based on Power Reference	1012
<i>Zhifu Wang, Jianping Xu, Yifan Wang, Yuxi Jing, and Xin Chen</i>	
Power Characteristic and Phase Difference Analysis of Double-Ended PS Applied to ICWPT System	1020
<i>Wenjing Tang and Liming Shi</i>	
Analysis of Transfer Characteristics of Magnetic-Valve-Type Current Transformer	1030
<i>Shaojie Liu, Siming Wei, Yingying Zhao, Yue Tian, Yubo Fan, Baichao Chen, Cuihua Tian, and Zhexuan Zhang</i>	
Transient EMI Analysis of a Submodule of Modular Multilevel Converters Based on Discontinuous Galerkin Time-Domain Methods	1038
<i>Xiaoping Sun, Jiawei Wang, Fang Zhuo, Yanmei Zhang, He Chen, and Jinghui Shao</i>	

Investigations of the Influences of Parasitic Inductance on Modular Multilevel Converters	1046
<i>Yantao Lou, Pengcheng Zhu, Yanmei Zhang, He Chen, Xiaoping Sun, and Jiawei Wang</i>	
Numerical Investigation on Frequency Dependence of Hysteresis Characteristics of Conducting Ferromagnetic Materials	1057
<i>Zhang Yubo, Liu Tianyi, Liao Zhenyu, Li Dong, and Chen Dezhi</i>	
Design and Research of Distributed Coil Magnetic Levitation Platform	1069
<i>Changzhou Jiang, Chaofan Du, and Zhengfeng Ming</i>	
Adaptive Fast Power Control of Voltage Controlled Inverter Based on Timed Power Disturbance	1076
<i>Han Feng, Zhang Xing, Wang Jilei, Fu Xinxin, and Zhan Xiangdui</i>	
Research on Signal Extraction and Control Strategy of Single-Phase PWM Rectifier in d-q Coordinate Frame	1087
<i>Lieqian Gong, Guanggang Fu, Xin Wang, Mengyang Tang, Wu Liao, and Yiru Miao</i>	
Loss Calculation and Deadtime Compensation for DPWMMIN in Voltage Source Inverter	1096
<i>Binbin Qiu, Huadong Zhang, and Guoyong Li</i>	
Single-Phase Grid-Connected Current Source Inverter Based on Control of DC-Link Current	1112
<i>Binbin Qiu, Huadong Zhang, and Guoyong Li</i>	
High Stability and Efficiency in Dual-Buck Inverter with Feedback Linearization Controller	1121
<i>Pingping Wen, Zengquan Yuan, Zhibao Yuan, and Haiping Xu</i>	
Electromagnetic Compatibility and Insulation Performance of UHVDC Converter Valve After Implanting Sensor Detectors	1129
<i>Zhiyao Luo, Siyuan Ma, Fei Du, Lei Shi, Shuai Yuan, and Tianyu Dong</i>	
Modeling and Parameter Sensitivity Analysis of Inductor Used Multi-material Powder Core	1136
<i>Yun Zhang, Zedong Zheng, Chi Li, and Qing Zhou</i>	
Optimized Design of T-type Three-Level Rectifier Based on Quasi-proportional Resonance Control	1150
<i>Kemin Dai, Jinwu Gong, Xiaolu Ge, Shangzhi Pan, and Xiaoming Zha</i>	

DC-Side Voltage Harmonic Control of a Three-Phase Current Source
Rectifier Under Unbalanced AC Voltage Conditions 1160
*Jixuan Zhang, Wenping Cao, Wenjie Zhu, Huajian Zhou,
and Cungang Hu*

Active Clamp Flyback Converter with Variable Resonant Modes 1170
Zhenye Dong, Qiang Zhang, Yuhui Yang, and Xueqin Zheng

Magnetic Field Analysis of Inter-turn Short Circuit Fault in Hollow
Reactor Based on Finite Element Simulation 1180
Jieyi Luo, Yuanjia Li, and Rongfu Zhong

Author Index 1191



Quadrature Six-Coils Wireless Charging with High Misalignment Tolerance and Constant Voltage Output

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Abstract. Aiming at improving the operating range of the wireless charging system with misalignment tolerance, a design method based on parameter optimization of wireless charging with wide range misalignment and constant-voltage output was proposed. The mathematical model of the proposed six-coils hybrid compensation network were established, and the output characteristics between load and mutual inductances were analyzed. The DD2Q (Double-D Quadrature) pad was proposed, which is beneficial to eliminate cross coupling and realize independent output of each channel. The results show that the system output current deviation is less than 5% when the coupling pads vary from 20 mm to 140 mm, and the efficiency is up to 94%.

Keywords: Wireless charging · Misalignment tolerance · Constant voltage output

1 Introduction

Inductive Power Transfer (IPT) is a method of energy transmission through high-frequency alternating magnetic field coupling, which has the advantages of safety, reliability, environmental friendliness and convenient operation. At present, it has been successfully applied to electronic products, medical electronic equipment and electric vehicles. Coupling coil is an important element of wireless charging system. The misalignment between the coupling coil will decrease the output power and efficiency. Therefore, wide range anti-offset output capability has become an important indicator of wireless charging system [1–5].

Aiming at improving the anti-offset ability, the optimization design is mainly from closed-loop control, magnetic coupling structure and high-order compensation network [6, 7]. The anti-offset output system based on closed-loop control usually requires additional wireless communication devices, but the wireless communication delay will

reduce the dynamic response of the system. DDQ coil structure, DD coil structure, I-type transmitting coil structure and 3D orthogonal coil structure were proposed in [8–11] to provide misalignment tolerance against coupling fluctuations. For example, a I-type transmitting coil is proposed in [9] to realize the fluctuation range of output voltage within 30% when the maximum offset in x direction is within 50%. A 3D orthogonal coil structure was presented in [11] to realize all-directional wireless charging, but the overall efficiency of the system is only 60%. Meanwhile, hybrid compensation network can also be used to provide better misalignment tolerance. A hybrid compensation network combining with LCC-LCC and S-S compensation network [12], could realize stable the power output when the system coupling coefficient varied from 0.2 to 0.3. However, this hybrid topology cannot operate without the secondary side. A series hybrid topology with the integrating compensating inductor into coupling coil was proposed in [13] to overcome the above mentioned issues. The operating principle of the hybrid compensation network was summarized in [14], and set up an experimental platform, which could limit the fluctuation range, when the coupling coefficient is 0.08–0.16. To sum up, the existing methods can achieve anti-offset wireless charging, but the range of coupling coefficient is relatively narrow. Considering different EVs, such as family cars, SUVs or trucks, the vertical height of the coupling coil is different, and the coupling coefficient varies widely, resulting in transmission power fluctuation and efficiency decline. Therefore, it is necessary to improve the operating range of vertical misalignment tolerance.

The six-coil hybrid topology is presented in this paper. Firstly, the output characteristics of the topological circuit are analyzed. Secondly, the magnetic coupling coil structure of DD2Q is proposed to realize the mutual inductance decoupling between the same side coils. Finally, the experimental results show that the six-coil hybrid topology can achieve a wide range of anti-offset constant-current output, and the maximum efficiency of the system can reach 94%.

2 The Proposed Hybrid IPT System

Figure 1 illustrates the six-coil hybrid topology circuit. Aiming at minimizing the VA rating, all resonant components should be tuned to the same angle frequency ω , therefore, we can get

$$\begin{cases} \omega^2 L_0 C_0 = \omega^2 L_1 \frac{C_0 C_1}{C_0 + C_1} = 1, \omega^2 L_7 C_7 = \omega^2 L_4 \frac{C_4 C_7}{C_4 + C_7} = 1 \\ \omega^2 L_2 C_2 = \omega^2 L_3 C_3 = \omega^2 L_6 C_6 = 1, \omega^2 L_8 C_8 = \omega^2 L_5 \frac{C_5 C_8}{C_5 + C_8} = 1 \end{cases} \quad (1)$$

Then, the KVL equations can be obtained as

$$\begin{bmatrix} Z_{00} & Z_{01} & Z_{02} & 0 & Z_{04} & 0 & 0 \\ Z_{10} & Z_{11} & Z_{12} & 0 & Z_{14} & 0 & Z_{16} \\ Z_{20} & Z_{21} & Z_{22} & 0 & 0 & Z_{25} & Z_{26} \\ 0 & 0 & 0 & Z_{33} & 0 & Z_{35} & 0 \\ Z_{40} & Z_{41} & 0 & 0 & Z_{44} & 0 & Z_{46} \\ 0 & 0 & Z_{52} & Z_{53} & 0 & Z_{55} & Z_{56} \\ 0 & Z_{61} & Z_{62} & 0 & Z_{64} & Z_{65} & Z_{66} \\ 0 & 0 & Z_{72} & 0 & 0 & 0 & Z_{75} \end{bmatrix} \begin{bmatrix} \dot{I}_0 \\ \dot{I}_1 \\ \dot{I}_2 \\ \dot{I}_3 \\ \dot{I}_4 \\ \dot{I}_5 \\ \dot{I}_7 \end{bmatrix} = \begin{bmatrix} \dot{U}_{out} \\ 0 \\ 0 \\ \dot{U}_{out} \\ 0 \\ 0 \\ 0 \\ \dot{U}_{AC} \end{bmatrix} \quad (2)$$

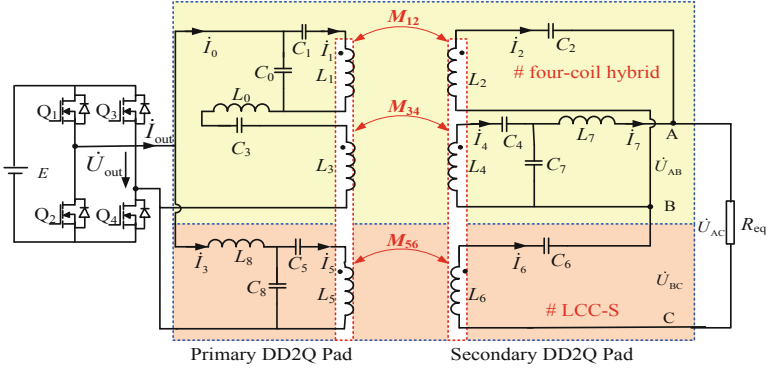


Fig. 1. Proposed six-coil hybrid IPT system.

where $Z_{00} = j\omega L_0 + (j\omega C_0)^{-1} + j\omega L_3 + (j\omega C_3)^{-1}$, $Z_{01} = Z_{10} = -(j\omega C_0)^{-1}$, $Z_{02} = Z_{20} = -j\omega M_{23}$, $Z_{04} = Z_{40} = -j\omega M_{34}$, $Z_{11} = j\omega L_1 + (j\omega C_0)^{-1} + (j\omega C_1)^{-1}$, $Z_{12} = Z_{21} = -j\omega M_{12} - j\omega M_{16}$, $Z_{14} = Z_{41} = -j\omega M_{14}$, $Z_{16} = Z_{61} = -j\omega M_{16}$, $Z_{22} = j\omega L_2 + (j\omega C_2)^{-1} + R_{AC} + j\omega L_6 + (j\omega C_6)^{-1}$, $Z_{25} = Z_{52} = -j\omega M_{25} - j\omega M_{56}$, $Z_{26} = Z_{62} = R_{AC} + j\omega L_6 + (j\omega C_6)^{-1}$, $Z_{33} = j\omega L_8 + (j\omega C_8)^{-1}$, $Z_{35} = Z_{53} = -(j\omega C_8)^{-1}$, $Z_{44} = j\omega L_4 + (j\omega C_4)^{-1} + (j\omega C_7)^{-1}$, $Z_{46} = Z_{64} = -(j\omega C_7)^{-1}$, $Z_{55} = j\omega L_5 + (j\omega C_5)^{-1} + (j\omega C_8)^{-1}$, $Z_{56} = Z_{65} = -j\omega M_{56}$, $Z_{66} = j\omega L_7 + (j\omega C_7)^{-1} + R_{AC} + j\omega L_6 + (j\omega C_6)^{-1}$, $Z_{72} = Z_{76} = R_{AC}$.

In this paper, only the main mutual inductance is considered and the cross mutual inductance is ignored. Thus, we can get,

$$\dot{U}_{AC} = \frac{L_7 M_{12} \dot{U}_{out}}{L_0 L_7 + M_{12} M_{34}} + \frac{M_{56} \dot{U}_{out}}{L_8} \quad (3)$$

From (3), the output voltage of the load is related with resonant inductor L_0 , L_7 , L_8 . If these parameters are well designed, the proposed IPT system can maintain stable voltage output.

3 Magnetic Coupler

Figure 2 shows the DD2Q pad in this paper, and the Magnetic inductance distribution is shown in Fig. 3. It is clear that the cross coupling occurs when the lateral misalignment happens, while there is only main coupling when the vertical misalignment happens. Therefore, the proposed DD2Q can be used in these applications, such as medical implant and AGVs, which may has wide vertical misalignment.

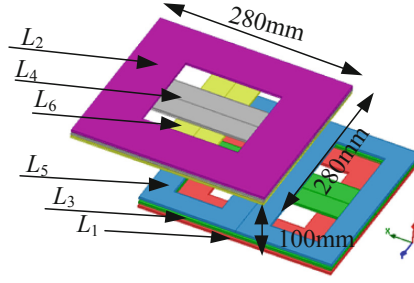


Fig. 2. DD2Q magnetic coupler

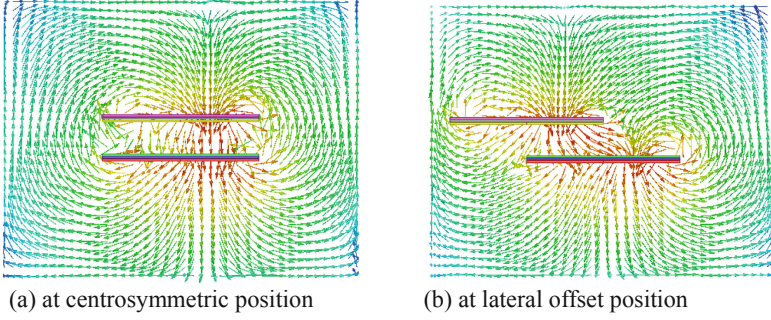


Fig. 3. Magnetic inductance distribution of the DD2Q coil structure

4 Experimental Verification

Figure 4 shows the wireless charging experiment platform, where the electronic load is used to simulate the changes in battery charging process. And Table 1 is the specific experimental parameters are shown in Table 1.

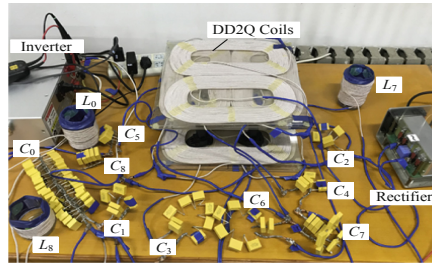
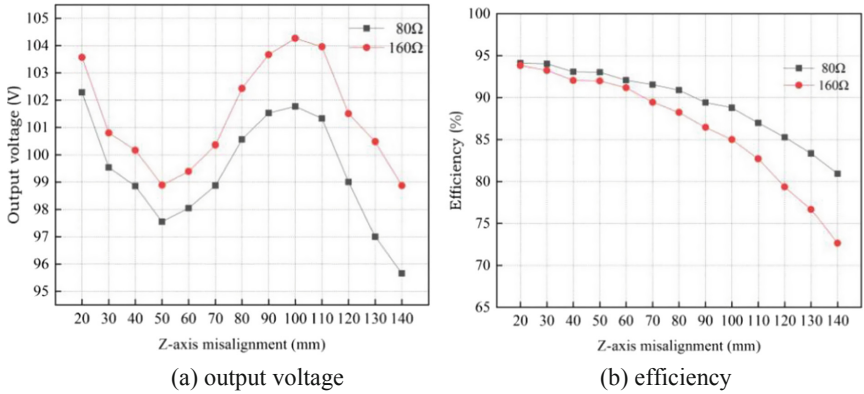


Fig. 4. Experiment platform

Figure 5(a) shows the output voltage curves with $80\ \Omega$ and $160\ \Omega$ load when vertical misalignment changes from 20 mm to 140 mm. It is obvious that the output voltage can remain relatively constant, The maximum output voltage is 104.5 V when the vertical

Table 1. The parameters

Parameter	Value	Parameter	Value
f	85 kHz	C_1	24.9 nF
L_1	150.1 μH	C_2	24.1 nF
L_2	149.8 μH	C_3	22.0 nF
L_3	160.1 μH	C_4	35.9 nF
L_4	160.2 μH	C_5	41.0 nF
L_5	160.1 μH	C_6	22.0 nF
L_6	160.1 μH	C_7	58.6 nF
L_7	60.2 μH	C_8	51.8 nF
L_8	70.2 μH	Air gap	20 mm–140 mm
C_0	388.4 nF	E	55 V

**Fig. 5.** Output voltage and efficiency curves at z-axis misalignment

misalignment reaches 100 mm, and the minimum output voltage is 95.66 V when the vertical misalignment reaches 140 mm. Figure 5(b) shows the system efficiency decreases when the vertical misalignment increases.

Figure 6 shows the experimental waveforms of different z-axis misalignment when the load resistance is 80 Ω . It can be obviously found that the variation of the output voltage is within 5%.

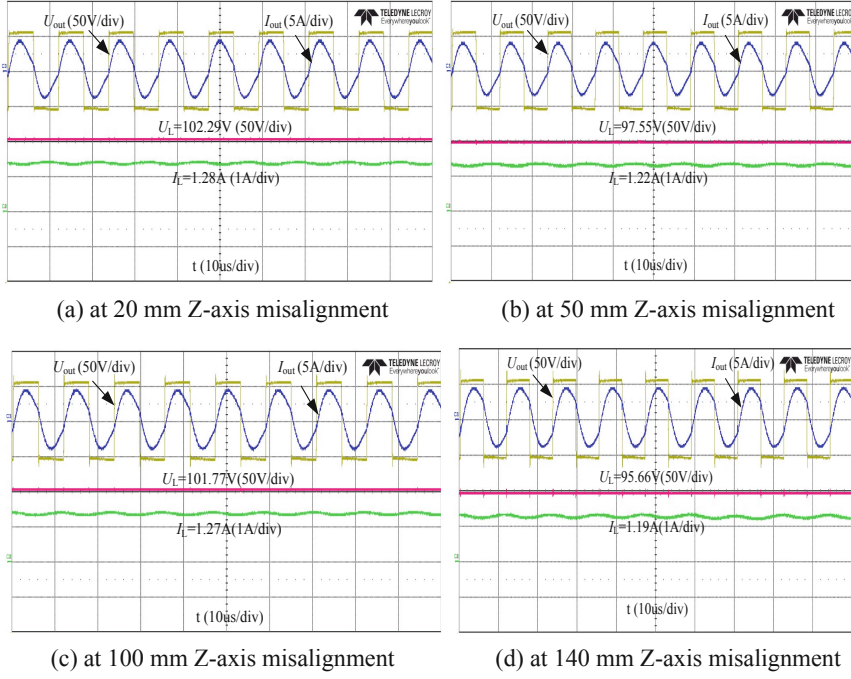


Fig. 6. Experimental waveforms at $R_L = 80 \Omega$

5 Conclusion

This paper presents a six-coil hybrid IPT topology. Firstly, the working characteristics of the system circuit are analyzed, and the variation rule of the output current is summarized. Secondly, DD2Q coupling coil structure is proposed to eliminate cross-coupling mutual inductance. Finally, the experimental results are consistent with the theoretical analysis.

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Inductively Coupled Power Transfer System Based Constant Voltage and Constant Current Charging for Rail Transit System

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Abstract. This paper focus on the constant voltage (CV) and constant current (CC) charging mode for rail transit energy storage by inductively coupled power transfer (ICPT) system. Firstly, the mathematical model of ICPT system based on LCC-S compensation network is established and analyzed, then a method of switching the parallel compensation capacitor of primary side to realize the switching of CV and CC charging mode is proposed in this paper, the zero voltage switching (ZVS) of MOSFETs can be realized in either CV or CC charging mode, and the method has the advantages of simple operation and high reliability. Finally, the simulation results are presented to verify the feasibility of the proposed method.

Keywords: Constant voltage · Constant current · Rail transit system · Inductively coupled power transfer system · Zero voltage switching

1 Introduction

At present, the third rail or overhead line and pantograph are the main power supply methods for rail transit system. However, these power supply methods have problems such as friction, electric sparks, electric shock risks and higher maintenance costs [1]. Therefore, the ICPT system has become an alternative to rail transit system power system power supply.

The LCC-S compensation network has better advantages for ICPT charging system, such as constant transmitting coil current, high efficiency and low losses [2]. Another advantage for its application in rail transit system is the reduction of the total weight of the vehicle, because only one compensation capacitor is needed.

The battery is the most commonly load as the energy storage in the rail transit system [3]. The battery charging process is mainly divided into two modes: CC charging mode and CV charging mode as shown in Fig. 1. First, the CC charging mode is used. When the battery voltage reaches the setting value, then the CV charging mode needs to be used. When the charging current is reduced to the charging cut-off current, the battery charging ends. The alternative CC and CV charging mode will prolong the

service life of the battery, and it is also important to the safety of the ICPT system. Therefore, it is necessary to switch between the CC charging mode and CV charging mode corresponding to the ICPT system used in the rail transit system.

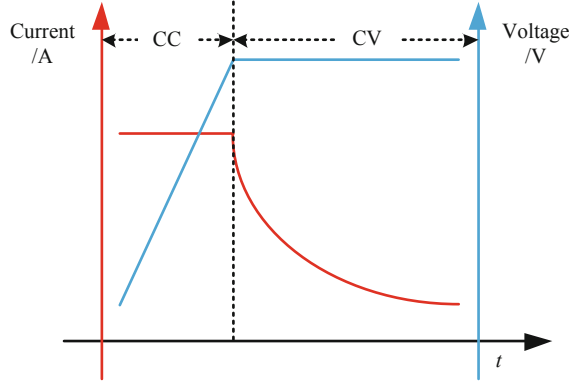


Fig. 1. Battery charging process.

In order to realize the switching of CV and CC charging mode of the ICPT system, a method of switching working frequency of the inverter is proposed in [4, 5]. This method doesn't require wireless communication, but this method is easy to cause the instability of the ICPT system with frequency bifurcation. In [6, 7], the closed-loop control method is adopted to realize the CV or CC charging mode of ICPT system, but closed-loop control method needs to transmit the voltage or current signal to the primary side, the data signal may be interfered by the energy signal, which will affect control accuracy. Meanwhile, the stability of the system using the closed-loop control also needs further research. In [8–10], a method of changing primary side or secondary side compensation structure is adopted, but more switching devices and compensation devices are used in this method, and the switching process between CV and CC charging mode is more complex.

In this paper, the ICPT system based on LCC-S compensation network is researched. First, the mathematical model of the system is established, and the conditions for the system to realize the CV and CC mode are obtained through analysis. Then, the method of switching parallel compensation capacitor on the primary side is proposed, the ZVS of the MOSFETs can be realized. Finally, the feasibility of the proposed method is verified through simulation results.

2 Topology of ICPT System

The topology of ICPT system is shown in Fig. 2. V_{dc} is the input dc voltage, V_{ab} and V_{cd} are the input and output voltages of the compensation network, respectively, V_o is the output dc voltage, I_1 is the input current of the compensation network, I_p and I_s are the current of the transmitting coil and receiving coil, respectively. L , C , C_1 , C_p and L_p are formed primary side of compensation network while L_s and C_s are formed secondary

side of the compensation network. r_p and r_s are the inner resistance, M is the mutual inductance, C_o is the output capacitor, R is the load, $S_1 \sim S_4$ are the MOSFETs of the inverter, $D_1 \sim D_4$ are the diodes of the rectifier.

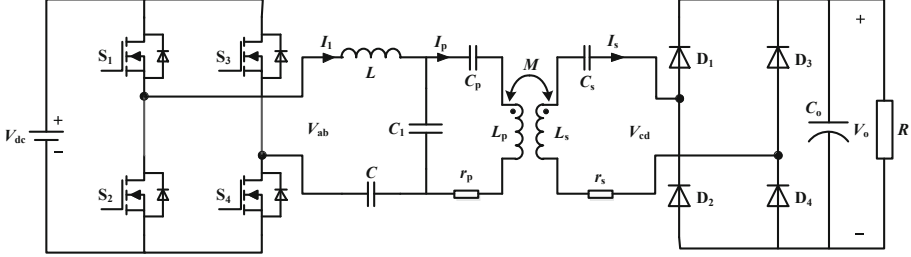


Fig. 2. Topology of ICPT system.

If r_p and r_s are ignored, the equivalent circuit of the ICPT system is shown in Fig. 3. Each parameter in Fig. 3 is expressed as (1).

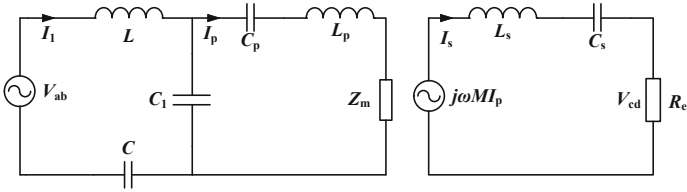


Fig. 3. Equivalent circuit of the ICPT system.

$$\begin{cases} V_{ab} = 2\sqrt{2}V_{dc}/\pi \\ Z_m = (\omega M)^2/(R_e + j\omega L_s + 1/j\omega C_s) \\ R_e = 8R/\pi^2 \\ V_{cd} = 2\sqrt{2}V_o/\pi \end{cases} \quad (1)$$

where ω is the resonant angular frequency of the system, Z_m is the reflection impedance, R_e is the ac equivalent resistance.

Let $Z_{eq} = j\omega L + 1/j\omega C$, $Z_C = 1/j\omega C_1$, $Z_p = j\omega L_p + 1/j\omega C_p$ and $Z_s = j\omega L_s + 1/j\omega C_s$, so the impedance of the primary side can be expressed as follows:

$$Z_{in} = Z_{eq} + Z_C/(Z_p + Z_m) = \frac{Z_{eq}(Z_C + Z_p + Z_m) + Z_C(Z_p + Z_m)}{Z_C + Z_p + Z_m} \quad (2)$$

So, I_1 , I_p , I_s and V_{cd} can be expressed as follows,

$$I_1 = \frac{V_{ab}}{Z_{in}} = \frac{Z_C + Z_p + Z_m}{Z_{eq}(Z_C + Z_p + Z_m) + Z_C(Z_p + Z_m)} V_{ab} \quad (3)$$

$$I_p = \frac{Z_C}{Z_C + Z_p + Z_m} I_1 = \frac{Z_C}{Z_{eq}(Z_C + Z_p + Z_m) + Z_C(Z_p + Z_m)} V_{ab} \quad (4)$$

$$I_s = \frac{j\omega M}{Z_s + R_e} I_p = \frac{j\omega M Z_C}{(Z_s + R_e)Z_{eq}(Z_C + Z_p + Z_m) + (Z_s + R_e)Z_C(Z_p + Z_m)} V_{ab} \quad (5)$$

$$V_{cd} = I_s R_e = \frac{j\omega M Z_C R_e}{(Z_s + R_e)Z_{eq}(Z_C + Z_p + Z_m) + (Z_s + R_e)Z_C(Z_p + Z_m)} V_{ab} \quad (6)$$

3 Analysis of CV and CC Charging Mode

3.1 CV Charging Mode

When the conditions shown in (7) are satisfied by the ICPT system, the CV charging mode of the ICPT system can be realized.

$$\begin{cases} Z_{eq} + Z_C = 0 \\ Z_p + Z_C = 0 \\ Z_s = 0 \end{cases} \quad (7)$$

So, the impedance of the system in CV charging mode can be expressed as:

$$Z_{in_CV} = \frac{Z_C Z_p}{Z_m} = \frac{R_e}{(\omega^2 M C)^2} \quad (8)$$

It can be seen from (8), the impedance Z_{in_CV} is resistive. In order to realize ZVS of MOSFETs, the impedance of the system needs to be designed to be slightly inductive.

In CV charging mode, V_{cd} can be expressed as follows:

$$V_{cd} = \frac{\omega M}{\omega L_p - 1/\omega C_p} V_{ab} \quad (9)$$

The curves of V_{cd} with operation frequency f under different load are shown in Fig. 4, and the ICPT system parameters are shown in Table. 1. As can be seen from Fig. 4, when the working frequency is 30 kHz, the CV charging mode of the ICPT system can be realized.

3.2 CC Charging Mode

On the basis of (5), I_s can be further derived as follows:

$$I_s = \frac{j\omega M Z_C}{(Z_s + R_e)[Z_{eq}(Z_C + Z_p) + Z_C Z_p] + (\omega M)^2 Z_{eq} + (\omega M)^2 Z_C} V_{ab} \quad (10)$$

When the condition shown in (11) is satisfied by the ICPT system, the CC charging mode of the ICPT system can be realized.

$$Z_{eq}(Z_C + Z_p) + Z_C Z_p = 0 \quad (11)$$

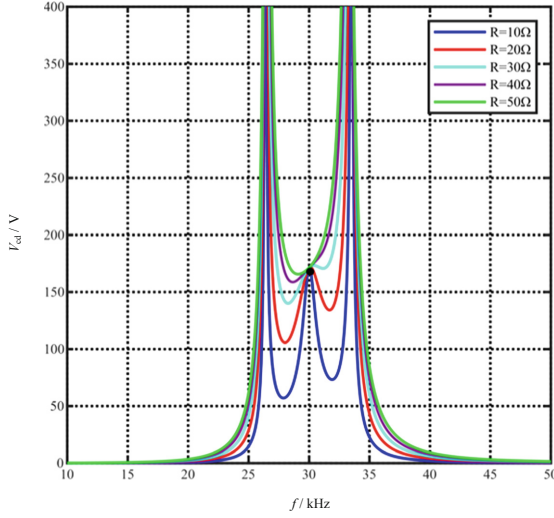


Fig. 4. Curves of V_{cd} with f under different load.

Table 1. Parameters of the ICPT system.

Symbol	Value	Symbol	Value
V_{dc}	100 V	L	62 μ H
C	0.52 μ F	C_1	3.57 μ F
L_p	22.14 μ H	C_p	1.97 μ F
r_p	0.033 Ω	L_s	980 μ H
C_s	28.71 nF	r_s	0.495 Ω
M	15 μ H	C_o	2000 μ F

To simplify the structure of the ICPT system, only one part of the system is modified in this paper, so there are three solutions are shown in (12), (13) and (14), respectively.

$$Z_C = -\frac{Z_{eq}Z_p}{Z_{eq} + Z_p} \quad (12)$$

$$Z_p = -\frac{Z_{eq}Z_C}{Z_{eq} + Z_C} \quad (13)$$

$$Z_{eq} = -\frac{Z_pZ_C}{Z_p + Z_C} \quad (14)$$

However, according to (7), in CV charging mode, $Z_{eq} + Z_C = 0$, $Z_p + Z_C = 0$, which will result in no solution to (13) and (14). Therefore, (12) is the only selection for the ICPT system to realize the CC charging mode in this paper.

So, on the basis of (7) and (12), in CC charging mode, the capacitance of the parallel compensation capacitor C_a can be derived as follows:

$$C_a = C_1 \quad (15)$$

So, the impedance of the system in CC charging mode can be expressed as:

$$Z_{in_CC} = \frac{-Z_C Z_m}{2Z_m - Z_C} = \frac{(\omega M)^2 R_e + j2\omega C_1 (\omega M)^4}{4(\omega C_1)^2 (\omega M)^4 + R_e^2} \quad (16)$$

It can be seen from (16), the impedance Z_{in_CC} is inductive, so ZVS of MOSFETs can be realized.

In CC charging mode, I_s can be expressed as:

$$I_s = -j \frac{V_{ab}}{\omega M} \quad (17)$$

The curves of I_s with operation frequency f under different load are shown in Fig. 5. As can be seen from Fig. 5, when parallel compensation capacitor C_a is added, when the working frequency is 30 kHz, the CC charging mode of the ICPT system can be realized.

Therefore, the topology of ICPT system that can switch between CV and CC charging mode is shown in Fig. 6. When switch S_a is turned off, the CV charging mode can be realized, when S_a is turned on, the CC charging mode can be realized.

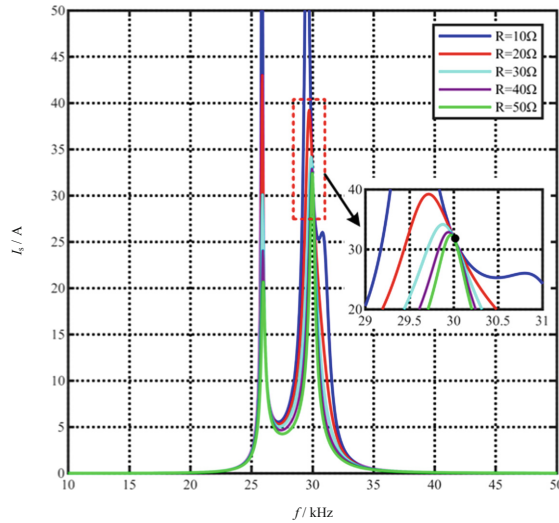


Fig. 5. Curves of I_s with f under different load.